EVALUATION KIT AVAILABLE

TC1027

Linear Building Block – Quad Low-Power Comparator and Voltage Reference

FEATURES

- Combines Four Comparators and a Voltage Reference in a Single Package
- Optimized for Single-Supply Operation
- Small Package ....16-Pin SOIC, QSOP, or DIP (Narrow)
- Ultra Low Input Bias Current ..... Less than 100 pA
- Low Quiescent Current .... 18 μA (Typ.)
- Rail-to-Rail Inputs and Outputs
- Operates Down to V_{DD} = 1.8V, Min

APPLICATIONS

- Power Management Circuits
- Battery Operated Equipment
- Consumer Products

GENERAL DESCRIPTION

The TC1027 is a mixed-function device combining four general purpose comparators and a voltage reference in a single 16-pin package.

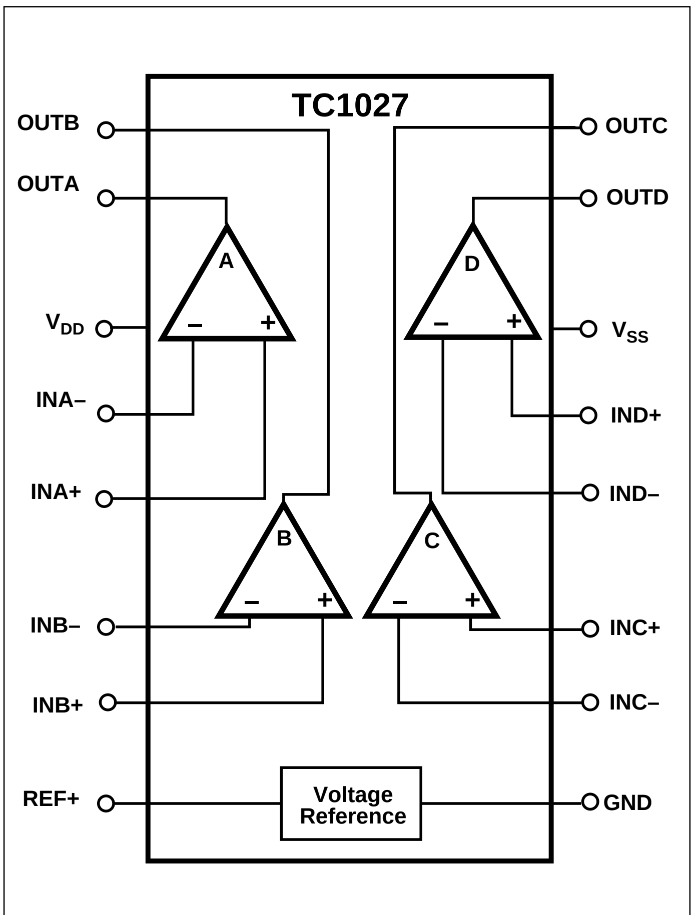
This increased integration allows the user to replace two packages, which saves space, lowers supply current, and increases system performance.

The TC1027 is optimized for low supply voltage and very low supply current operation (18 μA typ), making it ideal for battery-operated applications.

The comparators have rail-to-rail inputs and outputs which allows operation from low supply voltages with large input and output signal swings.

Packaged in a 16-Pin QSOP, 16-Pin SOIC (0.150 wide) or 16-pin DIP, the TC1027 is ideal for applications requiring high integration, small size, and low power.

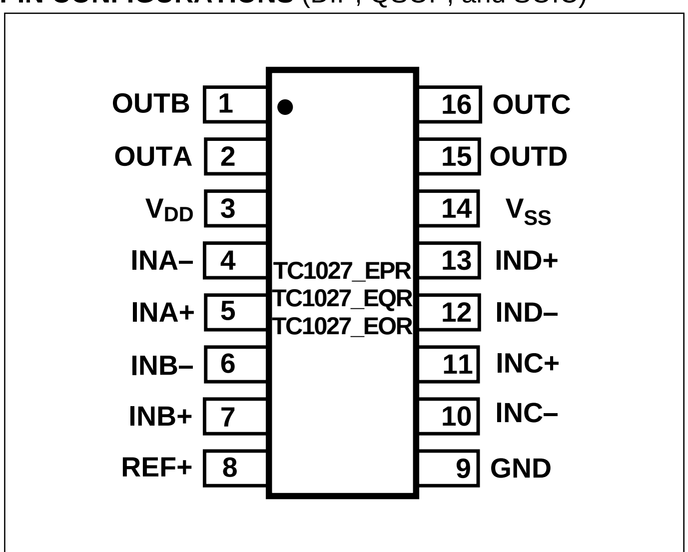
FUNCTIONAL BLOCK DIAGRAM



ORDERING INFORMATION

Part No.	Package	Temp. Range
TC1027CEPR	16-Pin DIP	– 40°C to +85°C
TC1027CEQR	16-Pin QSOP	– 40°C to +85°C
TC1027CEOR	16-Pin SOIC	– 40°C to +85°C
TC1043EV Evaluation Kit for Linear Building Block Family		

PIN CONFIGURATIONS (DIP, QSOP, and SOIC)



ABSOLUTE MAXIMUM RATINGS*

Supply Voltage 6.0V
Voltage on Any Pin:
(With Respect to Supplies) .. (V_{SS} – 0.3V) to (V_{DD} +0.3V)
Operating Temperature Range: .... – 40°C to + 85°C
Storage Temperature Range .... – 55°C to +150°C
Lead Temperature (Soldering, 10 sec) .... +260°C

* Static-sensitive device. Unused devices must be stored in conductive material. Protect devices from static discharge and static fields. Stresses above those listed under Absolute Maximum Ratings may cause permanent damage to the device. These are stress ratings only and functional operation of the device at these or any other conditions above those indicated in the operational sections of the specifications is not implied. Exposure to Absolute Maximum Rating Conditions for extended periods may affect device reliability.

ELECTRICAL CHARACTERISTICS: Typical values apply at 25°C and V_{DD} = 3.0V. Minimum and maximum values apply for T_A = –40° to +85°C, and V_{DD} = 1.8V to 5.5V, unless otherwise specified.

Symbol	Parameter	Test Conditions	Min	Typ	Max	Unit
V_{DD}	Supply Voltage		1.8	—	5.5	V
I_Q	Supply Current	All outputs unloaded	—	18	26	µA
Comparators						
V_{ICMR}	Common Mode Input Voltage Range		V_{SS} – 0.2	—	V_{DD} +0.2	V
V_{OS}	Input Offset Voltage	V_{DD} = 3V, V_{CM} =1.5V, T_A = 25°C T_A = –40°C to 85°C	–5 –5	—	+5 +5	mV mV
I_B	Input Bias Current	T_A = 25°C, IN+, IN– = V_{DD} to V_{SS}	—	—	±100	pA
V_{OH}	Output High Voltage	R_L = 10KΩ to V_{SS}	V_{DD} – 0.3	—	—	V
V_{OL}	Output Low Voltage	R_L = 10KΩ to V_{DD}	—	—	0.3	V
CMRR	Common Mode Rejection Ratio	T_A = 25°C, V_{DD} = 5V V_{CM} = V_{DD} to V_{SS}	66	—	—	dB
PSRR	Power Supply Rejection Ratio	T_A = 25°C, V_{CM} =1.2V V_{DD} = 1.8V to 5V	60	—	—	dB
I_{SRC}	Output Source Current	IN+ = $V_{DD,}$ IN– = V_{SS} Output Shorted to V_{SS} V_{DD} = 1.8V	1	—	—	mA
I_{SINK}	Output Sink Current	IN^+= $V_{SS,}$ IN^- = $V_{DD,}$ Output Shorted to V_{DD} V_{DD} = 1.8V	2	—	—	mA
t_{PD1}	Response Time	100 mV Overdrive,C_L = 100pF	—	4	—	µsec
t_{PD2}	Response Time	10 mV Overdrive, C_L = 100pF	—	6	—	µsec
Voltage Reference						
V_{REF}	Reference Voltage		1.176	1.200	1.224	V
$I_{REF(SOURCE)}$	Source Current		50	—	—	µA
$I_{REF(SINK)}$	Sink Current		50	—	—	µA
$C_{L(REF)}$	Load Capacitance		—	—	100	pF
N_{VREF}	Voltage Noise	100 Hz to 100 KHz	—	20	—	µVRMS
	Noise Density	1 KHz	—	1.0	—	$\mu V/\sqrt{Hz}$

DETAILED DESCRIPTION

The TC1027 is one of a series of very low-power, linear building block products targeted at low-voltage, single-supply applications. The TC1027 minimum operating voltage is 1.8V, and typical supply current is only 18 µA. It combines four comparators and a voltage reference in a single package.

Comparators

The TC1027 contains four comparators. The comparator's input range extends beyond both supply voltages by 200mV and the outputs will swing to within several millivolts of the supplies depending on the load current being driven.

The comparators exhibit a propagation delay and supply current which are largely independent of supply voltage. The low input bias current and offset voltage make them suitable for high impedance precision applications.

Voltage Reference

A 2.0 percent tolerance, internally biased, 1.20V bandgap voltage reference is included in the TC1027. It has a push-pull output capable of sourcing and sinking at least 50 µA.

GND (Pin 9) is connected to V_{SS} (Pin14) through the substrate of the integrated circuit. Large currents can flow between GND and V_{SS} if the pins are not at the same voltage.

TYPICAL APPLICATIONS

The TC1027 lends itself to a wide variety of applications, particularly in battery-powered systems. It typically finds application in power management, processor supervisory, and interface circuitry.

External Hysteresis (Comparator)

Hysteresis can be set externally with two resistors using positive feedback techniques (see Figure 1). The design procedure for setting external comparator hysteresis is as follows:

1. Choose the feedback resistor R_C. Since the input bias current of the comparator is at most 100 pA, the current through R_C can be set to 100 nA (i.e. 1000 times the input bias current) and retain excellent accuracy. The current through R_C at the comparator's trip point is V_R / R_C where V_R is a stable reference voltage.

2. Determine the hysteresis voltage (V_{HY}) between the upper and lower thresholds.

3. Calculate R_A as follows.

$$R_A = R_C \left(\frac{V_{HY}}{V_{DD}}\right)$$

Equation 1.

4. Choose the rising threshold voltage for V_{SRC} (V_{THR}).

5. Calculate R_B as follows:

$$R_B = \frac{1}{\left[\left(\frac{V_{THR}}{(V_R * R_A)}\right) - \frac{1}{R_A} - \frac{1}{R_C}\right]}$$

Equation 2.

6. Verify the threshold voltages with these formulas:

V_{SRC} rising:

$$V_{THR} = (V_R)(R_A)\left[\left(\frac{1}{R_A}\right) + \left(\frac{1}{R_B}\right) + \left(\frac{1}{R_C}\right)\right]$$

Equation 3.

V_{SRC} falling:

$$V_{THF} = V_{THR} - \left[\frac{(R_A * V_{DD})}{R_C}\right]$$

Equation 4.

Precision Battery Monitor

Figure 2 is a precision battery low/battery dead monitoring circuit. Typically, the battery low output warns the user that a battery dead condition is imminent. Battery dead typically initiates a forced shutdown to prevent operation at low internal supply voltages (which can cause unstable system operation).

The circuit of Figure 2 uses a single TC1027, one additional op amp, and only six external resistors. AMP 1 is a simple buffer while CMPTR1 and CMPTR2 provide precision voltage detection using V_R as a reference. Resistors R2 and R4 set the detection threshold for $\overline{\text{BATT LOW}}$ while resistors R1 and R3 set the detection threshold for $\overline{\text{BATT FAIL}}$. The component values shown assert $\overline{\text{BATT LOW}}$ at 2.2V (typical) and $\overline{\text{BATT FAIL}}$ at 2.0V (typical). Total current consumed by this circuit is typically 24 µA at 3V. Resistors R5 and R6 provide hysteresis for comparators CMPTR1 and CMPTR2, respectively.

32.768 KHz 'Time Of Day Clock' Crystal Controlled Oscillator

A very stable oscillator driver can be designed by using a crystal resonator as the feedback element. Figure 3 shows a typical application circuit using this technique to develop a clock driver for a Time Of Day (TOD) clock chip. The values of R_A and R_B determine the DC voltage level at which the comparator trips — in this case one-half of V_{DD}. The RC time constant of R_C and C_A should be set several times greater than the crystal oscillator's period, which will ensure a 50% duty cycle by maintaining a DC voltage at the inverting comparator input equal to the absolute average of the output signal.

Non-Retriggerable One Shot Multivibrator

Using two comparators, a non-retriggerable one shot multivibrator can be designed using the circuit configuration of Figure 4. A key feature of this design is that the pulse width is independent of the magnitude of the supply voltage because the charging voltage and the intercept voltage are a fixed percentage of V_{DD}. In addition, this one shot is capable of pulse width with as much as a 99% duty cycle and exhibits input lockout to ensure that the circuit will not re-trigger before the output pulse has completely timed out. The trigger level is the voltage required at the input to raise the voltage at node A higher than the voltage at node B, and is set by the resistive divider R4 and R10 and the impedance network composed of R1, R2, and R3. When the one shot has been triggered, the output of CMPTR2 is high, causing the reference voltage at the non-inverting input of CMPTR1 to go to V_{DD}. This prevents any additional input pulses from disturbing the circuit until the output pulse has timed out.

The value of the timing capacitor C1 must be small enough to allow CMPTR1 to discharge C1 to a diode voltage before the feedback signal from CMPTR2 (through R10) switches CMPTR1 to its high state and allows C1 to start an exponential charge through R5. Proper circuit action depends upon rapidly discharging C1 through the voltage set by R6, R9, and D2 to a final voltage of a small diode drop. Two propagation delays after the voltage on C1 drops below the level on the non-inverting input of CMPTR2, the output of CMPTR1 switches to the positive rail and begins to charge C1 through R5. The time delay which sets the output pulse width results from C1 charging to the reference voltage set by R6, R9, and D2, plus four comparator propagation delays. When the voltage across C1 charges beyond the reference, the output pulse returns to ground and the input is again ready to accept a trigger signal.

Oscillators and Pulse Width Modulators

Microchip's linear building block comparators adapt well to oscillator applications for low frequencies (less than 100 KHz). Figure 5 shows a symmetrical square wave generator using a minimum number of components. The output is set by the RC time constant of R4 and C1, and the total hysteresis of the loop is set by R1, R2, and R3. The maximum frequency of the oscillator is limited only by the large signal propagation delay of the comparator in addition to any capacitive loading at the output which degrades the slew rate.

To analyze this circuit, assume that the output is initially high. For this to occur, the voltage at the inverting input must be less than the voltage at the non-inverting input. Therefore, capacitor C1 is discharged. The voltage at the non-inverting input (V_H) is:

$$V_H = \frac{R2(V_{DD})}{[R2 + (R1 \,||\, R3)]}$$

Equation 5.

where, if R1 = R2 = R3, then:

$$V_H = \frac{2\,(V_{DD})}{3}$$

Equation 6.

Capacitor C1 will charge up through R4. When the voltage at the comparator's inverting input is1 equal to V_H, the comparator output will switch. With the output at ground potential, the value at the non-inverting input terminal (V_L) is reduced by the hysteresis network to a value given by:

$$V_L = \frac{V_{DD}}{3}$$

Equation 7.

Using the same resistors as before, capacitor C1 must now discharge through R4 toward ground. The output will return to a high state when the voltage across the capacitor has discharged to a value equal to V_L. The period of oscillation will be twice the time it takes for the RC circuit to charge up to one half its final value. The period can be calculated from:

$$\frac{1}{FREQ} = 2\,(0.694)\,(R4)\,(C1)$$

Equation 8.

The frequency stability of this circuit should only be a function of the external component tolerances.

Figure 6 shows the circuit for a pulse width modulator circuit. It is essentially the same as in Figure 5 with the addition of an input control voltage. When the input control voltage is equal to one-half V_{DD}, operation is basically the same as described for the free-running oscillator. If the input control voltage is moved above or below one-half V_{DD}, the duty cycle of the output square wave will be altered. This is because the addition of the control voltage at the input has now altered the trip points. The equations for these trip points are shown in Figure 6 (see V_H and V_L).

Pulse width sensitivity to the input voltage variations can be increased by reducing the value of R6 from 10 KΩ and conversely, sensitivity will be reduced by increasing the value of R6. The values of R1 and C1 can be varied to produce the desired center frequency.

EVALUATION KIT

The TC1043EV consists of a four-inch by six-inch pre-wired application circuit board. Pre-configured circuits include a pulse width modulator, wake-up timer, function generator, and others. On-board current meter terminals, voltage regulator, and a user-prototyping area speed circuit development. Please contact your local Microchip Technology representative for more information.

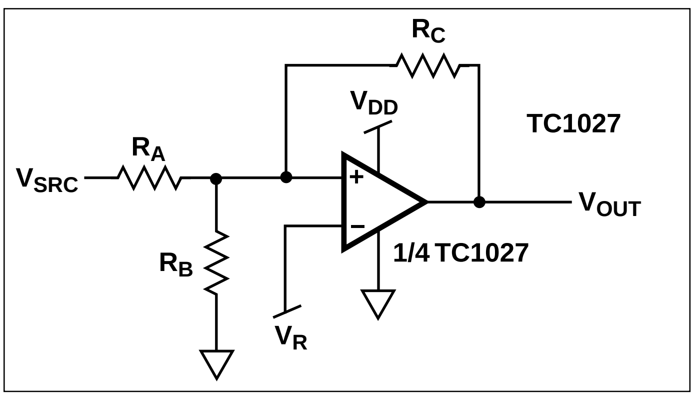


Figure 1. Comparator External Hysteresis

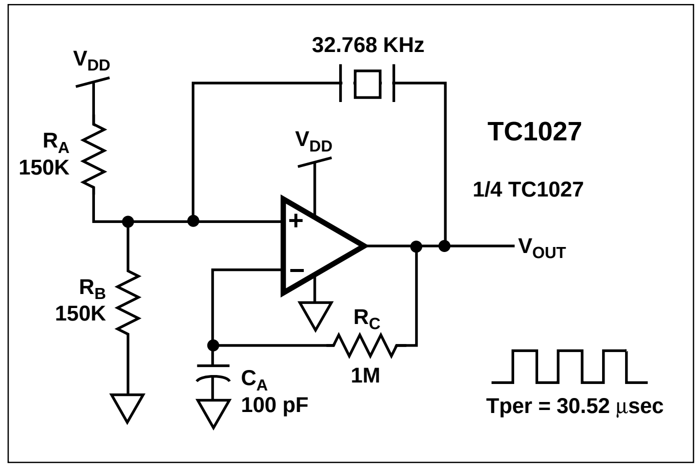


Figure 3. 32.768 KHz "Time of Day" Clock Oscillator

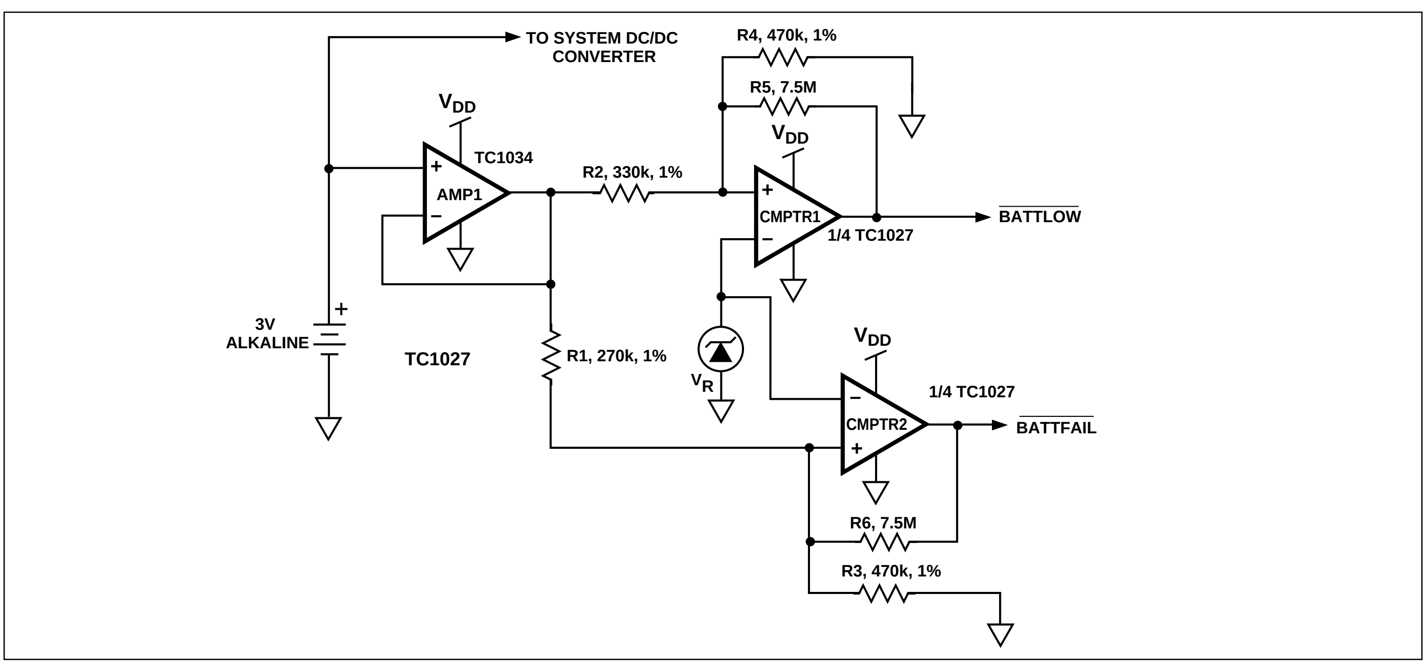


Figure 2. Precision Battery Monitor

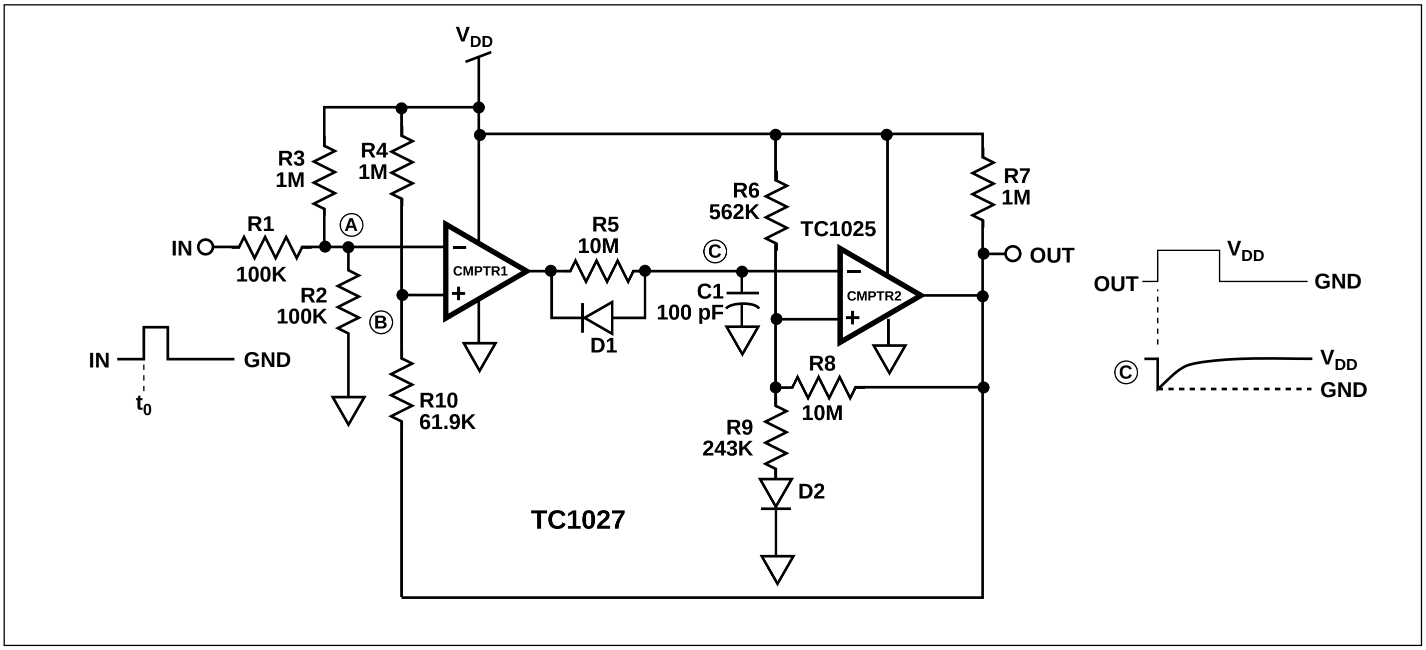
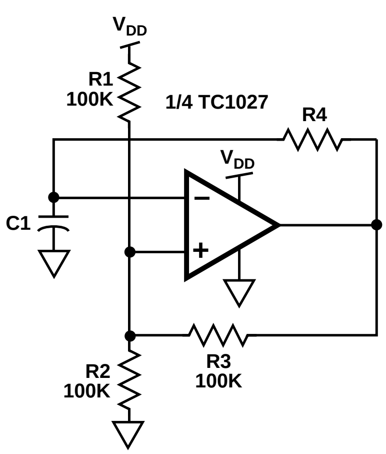


Figure 4. Non-Retriggerable Multivibrator



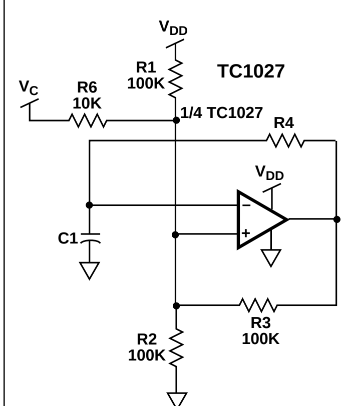
TC1027

$$V_H = \frac{R2\ (V_{DD})}{R2 + (R1||R3)}$$

$$V_L = \frac{(V_{DD})\ (R2||R3)}{R1 + (R2||R3)}$$

$$FREQ = \frac{1}{2(0.694)(R4)(C1)}$$

Figure 5. Square Wave Generator



$$V_H = \frac{V_{DD}\ (R_1R_2R_6 + R_2R_3R_6) + V_C\ (R_1R_2R_3)}{R_1R_2R_6 + R_1R_3R_6 + R_2R_3R_6 + R_1R_2R_3}$$

$$V_L = \frac{V_{DD}\ (R_2R_3R_6) + V_C\ (R_1R_2R_3)}{R_1R_2R_6 + R_1R_3R_6 + R_2R_3R_6 + R_1R_2R_3}$$

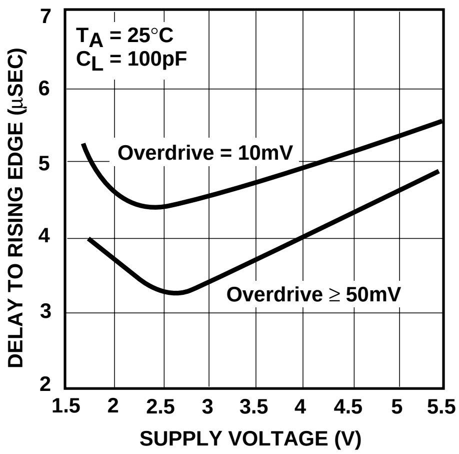
$$FREQ = \frac{1}{2\ (0.694)\ (R4)\ (C1)}$$

For Square Wave Generation,
Select R1= R2 = R3,
$V_C = \frac{V_{DD}}{2}$

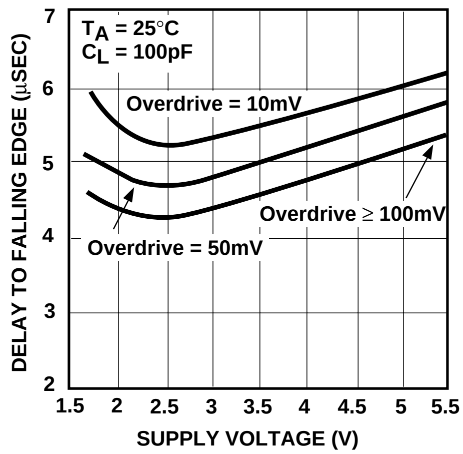
Figure 6. Pulse Width Modulator

TYPICAL CHARACTERISTICS

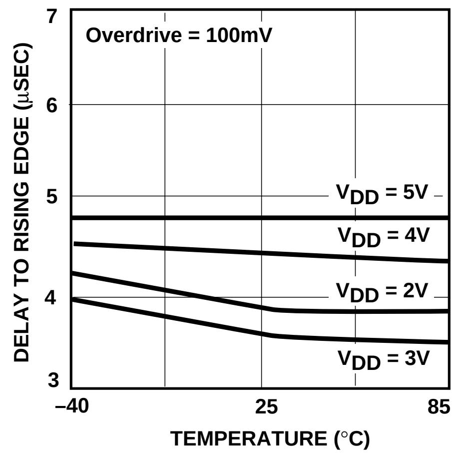
**Comparator
Propagation Delay vs. Supply Voltage**



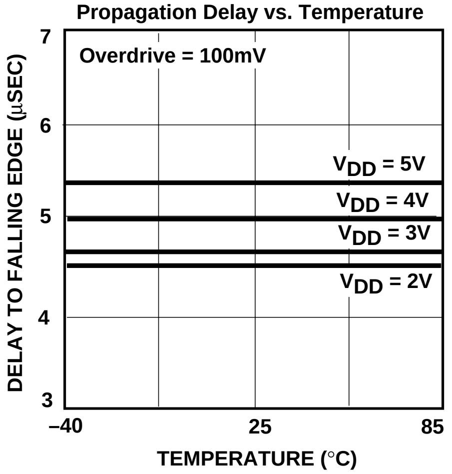
**Comparator
Propagation Delay vs. Supply Voltage**



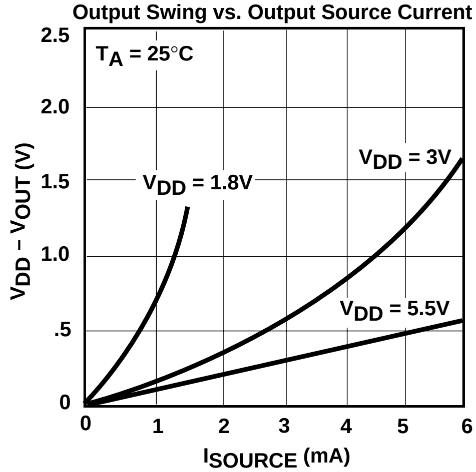
**Comparator
Propagation Delay vs. Temperature**



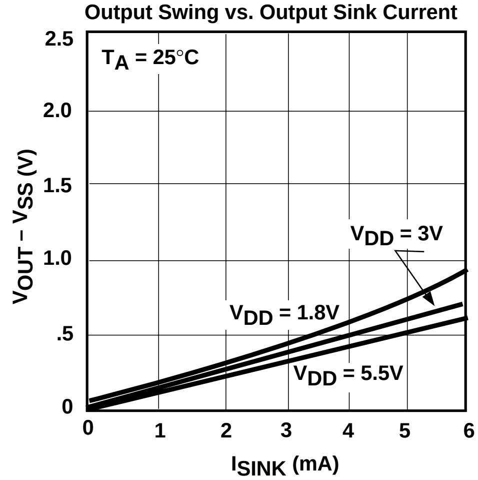
**Comparator
Propagation Delay vs. Temperature**



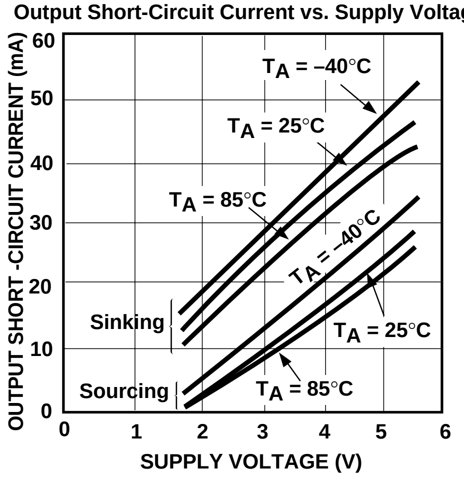
**Comparator
Output Swing vs. Output Source Current**



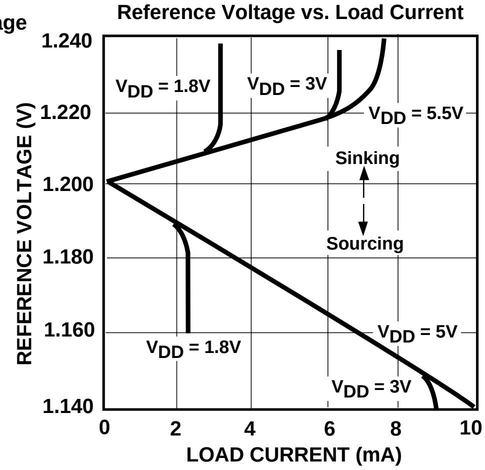
**Comparator
Output Swing vs. Output Sink Current**



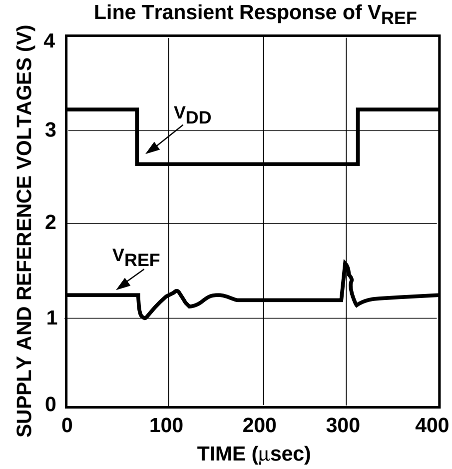
**Comparator
Output Short-Circuit Current vs. Supply Voltage**



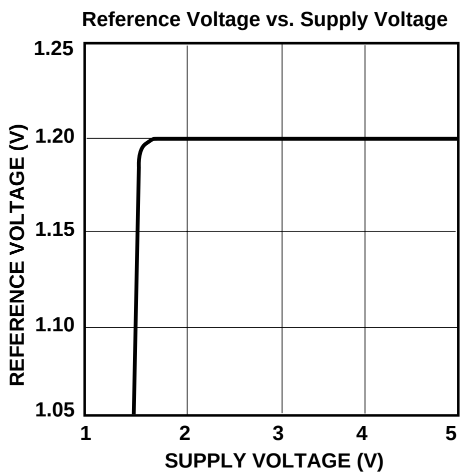
Reference Voltage vs. Load Current

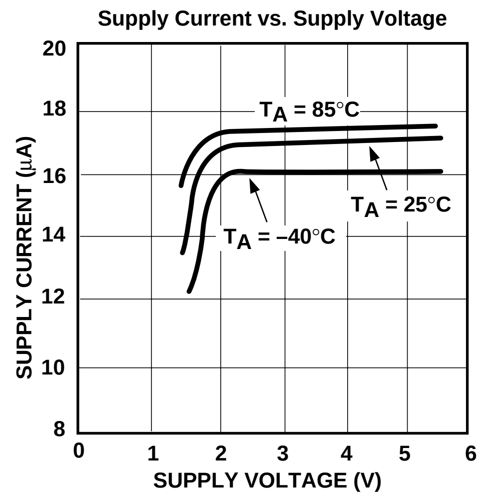


Line Transient Response of V_{REF}



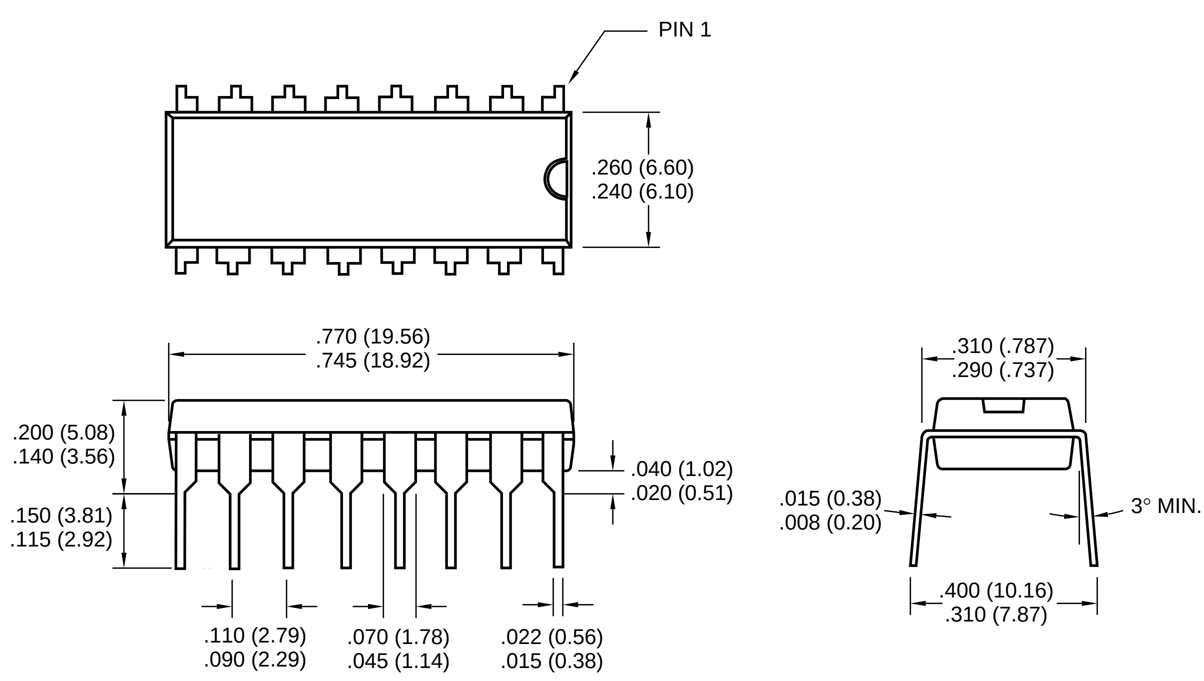
TYPICAL CHARACTERISTICS





PACKAGE DIMENSIONS

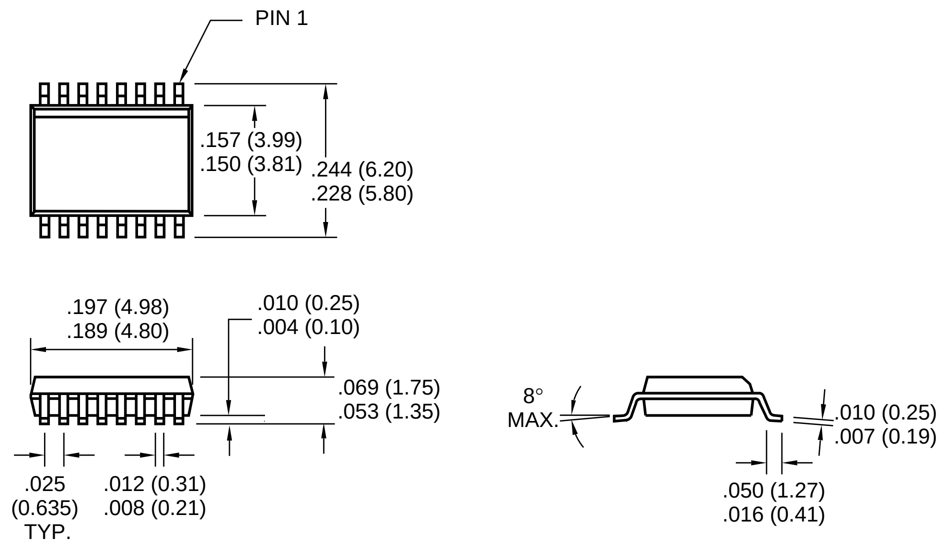
16-Pin Plastic DIP (Narrow)



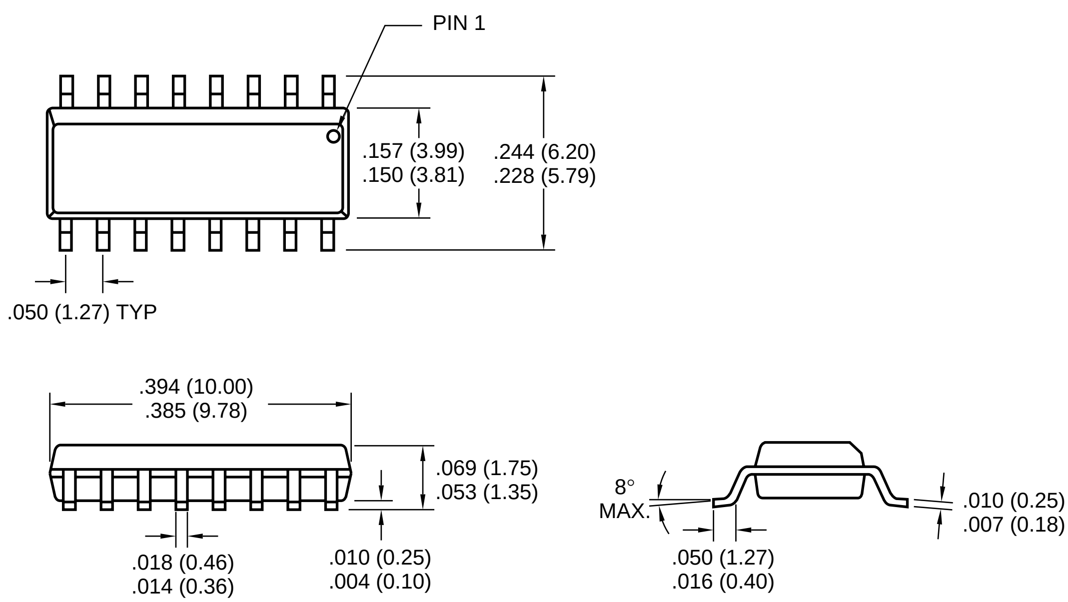
Dimensions: inches (mm)

PACKAGE DIMENSIONS CONT

16-Pin QSOP



16-Pin SOIC (Narrow)



Dimensions: inches (mm)

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New York
150 Motor Parkway, Suite 202
Hauppauge, NY 11788
Tel: 631-273-5305 Fax: 631-273-5335

San Jose
Microchip Technology Inc.
2107 North First Street, Suite 590
San Jose, CA 95131
Tel: 408-436-7950 Fax: 408-436-7955

Toronto
6285 Northam Drive, Suite 108
Mississauga, Ontario L4V 1X5, Canada
Tel: 905-673-0699 Fax: 905-673-6509

ASIA/PACIFIC

China - Beijing
Microchip Technology Beijing Office
Unit 915
New China Hong Kong Manhattan Bldg.
No. 6 Chaoyangmen Beidajie
Beijing, 100027, No. China
Tel: 86-10-85282100 Fax: 86-10-85282104

China - Shanghai
Microchip Technology Shanghai Office
Room 701, Bldg. B
Far East International Plaza
No. 317 Xian Xia Road
Shanghai, 200051
Tel: 86-21-6275-5700 Fax: 86-21-6275-5060

Hong Kong
Microchip Asia Pacific
RM 2101, Tower 2, Metroplaza
223 Hing Fong Road
Kwai Fong, N.T., Hong Kong
Tel: 852-2401-1200 Fax: 852-2401-3431

India
Microchip Technology Inc.
India Liaison Office
Divyasree Chambers
1 Floor, Wing A (A3/A4)
No. 11, OíShaugnessey Road
Bangalore, 560 025, India
Tel: 91-80-2290061 Fax: 91-80-2290062

Japan
Microchip Technology Intl. Inc.
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Kohoku-Ku, Yokohama-shi
Kanagawa, 222-0033, Japan
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Korea
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Samsung-Dong, Kangnam-Ku
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Singapore
Microchip Technology Singapore Pte Ltd.
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France
Arizona Microchip Technology SARL
Parc díActivite du Moulin de Massy
43 Rue du Saule Trapu
Batiment A - ler Etage
91300 Massy, France
Tel: 33-1-69-53-63-20 Fax: 33-1-69-30-90-79

Germany
Arizona Microchip Technology GmbH
Gustav-Heinemann Ring 125
D-81739 Munich, Germany
Tel: 49-89-627-144 0 Fax: 49-89-627-144-44

Germany
Analog Product Sales
Lochhamer Strasse 13
D-82152 Martinsried, Germany
Tel: 49-89-895650-0 Fax: 49-89-895650-22

Italy
Arizona Microchip Technology SRL
Centro Direzionale Colleoni
Palazzo Taurus 1 V. Le Colleoni 1
20041 Agrate Brianza
Milan, Italy
Tel: 39-039-65791-1 Fax: 39-039-6899883

United Kingdom
Arizona Microchip Technology Ltd.
505 Eskdale Road
Winnersh Triangle
Wokingham
Berkshire, England RG41 5TU
Tel: 44 118 921 5869 Fax: 44-118 921-5820

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